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## (54) Estimator of amplitude and frequency of a noisy biased sinusoid from short bursts of samples

Einrichtung zum Abschätzen der Amplitude und Frequenz eines verrauschten, vorgespannten Sinusoids aus kurzen Abtastblöcken

Dispositif d'estimation de l'amplitude et de la fréquence d'un signal sinusoïdal bruité et polarisé à partir de brefs paquets d'échantillons

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## (56) References cited:

EP-A- 0 058 050	EP-A- 0 107 884
EP-A- 0 371 192	EP-A- 0 454 946
GB-A- 2 160 983	US-A- 4 672 555

- IEEE TRANSACTIONS ON INSTRUMENTATION AND MEASUREMENT, vol. 41, no. 3, June 1992 US, pages 397-402, A.M.ZAYEZDNY ET AL. 'Short Time Measurement of Frequency and Amplitude in the Presence of Noise'
- INTERNATIONAL JOURNAL OF ELECTRONICS, vol. 69, no. 6, December 1990 LONDON GB, pages 747-765, A.I.ABU-EL-HAIJA 'Detecting the amplitude and frequency of noisy sinusoidal signals'
- ELECTRONIC DESIGN, vol. 38, no. 13, July 1990 US, pages 112-113, F.GOODENOUGH '8-Input, 8-Bit Watchdog Chip Monitors Systems'
- OLOFF H. AND HUETTERMANN J.: 'Radiation Damage in Solid 5-Halouracils. Free Radicals In Single Crystals of 5-Chlorouracil and 5-Chlorouridine' JOURNAL OF MAGNETIC RESONANCE vol. 27, 1977, pages 197 - 213

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**Description****BACKGROUND OF THE INVENTION**5    **1. Field of the Invention.**

[0001] The present invention relates generally to digital signal processing, and more particularly to signal processing for detecting the amplitude and frequency of a noisy, biased and sparsely-sampled sinusoidal signal.

10    **2. Background Art**

[0002] A known method of estimating the amplitude of a sampled sinusoidal signal is to compute a "root-mean square" (RMS) value, and then multiply the RMS value by the square root of two. This method, however, is inaccurate when the sinusoid is sparsely sampled and an estimate is obtained from a block of a small number of samples.

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**SUMMARY OF THE INVENTION**

[0003] In accordance with a basic aspect of the invention, there is provided a method of estimating the amplitude and frequency of a sinusoidal signal represented as sample values  $S_1, S_2, S_3, S_4$  at respective spaced instants in time. The method includes the steps of: computing a triplet of differences  $x_1, x_2, x_3$ , where  $x_1$  is a difference between  $S_2$  and  $S_1$ ,  $x_2$  is a difference between  $S_3$  and  $S_2$ , and  $x_3$  is a difference between  $S_4$  and  $S_3$ ; and computing an estimate (B) of the amplitude, and an estimate (f) of the frequency, of the sinusoidal signal from the triplet of differences. Preferably an indication of the estimate of the amplitude or frequency is computed as a ratio of algebraic functions of the differences  $x_1, x_2, x_3$ . The amplitude, for example, is computed as the square root of a first ratio of algebraic functions, and the frequency is computed as an arc-cosine function of a second ratio of algebraic functions. Preferably the ratio is evaluated by a division operation computed as a polynomial approximation, and the square root and the arc-cosine functions are also computed as polynomial approximations.

[0004] In accordance with another aspect, the present invention provides a method of obtaining an indication of a characteristic of a signal represented as sample values  $(x_1, x_2, x_3, \dots, x_n)$  at respective spaced instants in time. The method includes the steps computing a series of ratios of algebraic functions of triplets  $(x_i, x_{i+1}, x_{i+2})$  of neighboring ones of the sample values, and computing an average of the ratios to produce the indication of the signal characteristic. Preferably any ratio having a denominator value that has a magnitude less than a threshold value is excluded from the average of the ratios, so that the average will not be corrupted by any inaccurate result that could be obtained when dividing by a relatively small number.

[0005] In accordance with a final aspect, the present invention provides a system for monitoring the health of a plurality of analog signals in an electronic circuit. The system includes an analog multiplexer for scanning the analog signals, an analog-to-digital converter for converting a selected analog signal to a series of digital values, a programmed data processor, and an output unit for indicating an error condition to an operator. The data processor is programmed to operate the analog multiplexer and to receive and process the series of digital values from the analog-to-digital converter. In particular, the data processor is programmed to determine an indication of amplitude and an indication of frequency of each of the analog signals by computing ratios of algebraic functions of at least four samples in the respective series of digital values for each of the analog signals, and to compare the indication of amplitude and the indication of frequency to limit values to indicate the error condition when one of the indications of amplitude and frequency falls outside of boundaries set by the limit values.

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**BRIEF DESCRIPTION OF THE DRAWINGS**

[0006] Other objects and advantages of the present invention will become apparent upon reading the following detailed description and upon reference to the drawings, in which:

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FIG. 1 is a block diagram showing a first method of using the invention, wherein the amplitude and frequency of a sinusoidal signal is estimated in order to provide a predetermined correction for parasitic capacitance in a circuit; FIG. 2 is a block diagram showing a second method of using the invention, wherein a multiplexer scans a number of signals in a system, and the amplitude and frequency of each selected signal is estimated and compared to predetermined limits in order to monitor the health of the system;

FIG. 3 is a first portion of a flow diagram showing the present invention implemented for continuously estimating the amplitude and frequency of a sampled sinusoidal signal;

FIG. 4 is a second portion of a flow diagram showing the present invention implemented for continuously estimating

the amplitude and frequency of a sampled sinusoidal signal;

FIG. 5 is a third portion of a flow diagram showing the present invention implemented for continuously estimating the amplitude and frequency of a sampled sinusoidal signal; and

FIG. 6 is block diagram showing the present invention implemented for obtaining an estimate of amplitude and frequency from a block of samples of a sinusoidal signal.

[0007] While the invention will be described in connection with certain preferred embodiments, it is not intended that the invention should be limited to these particular embodiments. On the contrary, the invention is intended to include all modifications, alternatives, and equivalent arrangements as may be included within the scope of this invention as defined by the appended claims.

#### DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

[0008] Turning now to the drawings, there is shown in FIG. 1 a block diagram illustrating a first method of using the invention, wherein the amplitude and frequency of a sinusoidal signal is continuously estimated in order to provide a predetermined correction for parasitic capacitance in a circuit. In particular, FIG. 1 shows an angular rate sensor 10 excited by a sinusoidal drive signal  $v_d$  at a frequency  $f_o$ , and producing an output signal  $v_{do}$  indicating the level of excitation of the sensor, and a signal  $v_r$  including angular rate information. The angular rate information, however, appears as a double-sideband suppressed-carrier signal about a suppressed carrier at the frequency  $f_o$ . Such an angular rate sensor is described, for example, in Fersht et al. U.S. Patent 5,056,366 and Staudte U.S. Patent Re 32,931, herein incorporated by reference.

[0009] As shown in FIG. 1, the angular rate sensor 10 is excited by a driver circuit generally designated 11 so that the output signal  $v_{do}$  has a predetermined amplitude. For this purpose, the signal  $v_{do}$  is passed through a bandpass filter 12 to remove noise, and then the amplitude of the signal  $v_{do}$  is detected by an amplitude detector 13. An integrating comparator 14, having an associated input resistor 15 and a feedback capacitor 16, compares the amplitude of the signal  $v_{do}$  to a predetermined reference  $V_R$ , to produce an automatic gain control voltage  $V_{AGC}$ . The automatic gain control voltage  $V_{AGC}$  controls the gain of a variable-gain amplifier 17 to produce the exciting drive signal  $v_d$ .

[0010] To detect an angular rate signal  $\Omega$ , a demodulator circuit 18 includes a balanced modulator 19 that is excited at the frequency  $f_o$ . The balanced modulator 19 demodulates the signal  $v_r$  to produce a base-band signal that is lowpass filtered by a lowpass filter 20 to produce the angular rate signal  $\Omega$ .

[0011] Although not pertinent to the present invention, further details regarding the angular rate sensor 10, the driver 11, and the demodulator 18 can be found in U.S. Patent 53 610 36 issued Nov. 1, 1994, [Docket No. 92E083] by the present inventor Stanley A. White, and entitled "COMPLEX DIGITAL DEMODULATOR EMPLOYING CHEBYCHEV-APPROXIMATION DERIVED SYNTHETIC SINUSOID GENERATION."

[0012] In practice, the detected angular rate signal  $\Omega$  is a function of the amplitude of the drive signal  $v_d$ . Although the variation in the detected angular rate signal  $\Omega$  with respect to the amplitude of the drive signal  $v_d$  is rather small, it is significant for some applications, and it is practical to remove the variation by employing the present invention to estimate the amplitude of the drive signal  $v_d$ . For example, the variation in the detected angular rate signal  $\Omega$  with respect to the amplitude of the drive signal  $v_d$  can be considered to be caused by a parasitic capacitance  $C_p$  between nodes 19 and 20 in FIG. 1. In this case, the error  $\epsilon$  in the detected angular rate signal  $\Omega$  is approximately:

$$\epsilon = KAf_o \quad (\text{Equation 1})$$

[0013] where  $K$  is a predetermined constant,  $A$  is the amplitude of the drive signal  $v_d$ , and  $f_o$  is the frequency of the drive signal. The constant  $K$  is on the order of  $2\pi C_p Z_{in} G$ , where  $C_p$  is value of the parasitic capacitance,  $Z_{in}$  is the impedance at the node 22, and  $G$  is the conversion gain of the demodulator 18.

[0014] In accordance with an aspect of the present invention, the error  $\epsilon$  is determined by estimating at least the amplitude  $A$  of the drive signal  $v_d$ , as further described below. The frequency  $f_o$  could also be estimated, but since the frequency  $f_o$  is relatively constant in comparison to the amplitude  $A$  of the drive signal  $v_d$ , the frequency  $f_o$  need not be estimated, and instead could be assumed to be a fixed, nominal value. The amplitude and/or frequency of the drive signal  $v_d$  is estimated by sampling the drive signal with an analog-to-digital converter 23, and processing the samples in an amplitude and frequency estimator 24. The amplitude and frequency estimator 24 will be further described below with reference to FIGS. 3 to 6. A correction signal generator 25 generates a correction signal  $\epsilon_s$  based on the estimated amplitude and/or frequency, and an adder unit 26 subtracts the correction signal  $\epsilon_s$  from the angular rate signal  $\Omega$  to produce a corrected angular rate signal  $\Omega'$ .

[0015] Turning now to FIG. 2, there is shown a block diagram illustrating a second method of the invention, wherein

an analog multiplexer 30 scans a number of signals  $S^1, S^2, S^3, \dots, S^n$  from a system 31, and the amplitude and frequency of each selected signal is estimated and compared to predetermined limits in order to monitor the health of the system. The system 31, for example, is an inertial measurement unit including three angular rate sensors as described above with reference to FIG. 1, each of the angular rate sensors have an associated driver circuit and detector circuit, and each of the angular rate sensors sense the angular rate of rotation about a respective one of three orthogonal axes. In this case the signal  $S^i$  could be the drive signal  $v_d$  for the  $i$ th one of the angular rate sensors, and the amplitude and/or frequency estimate for each of the drive signals could also be used for correction of the angular rate signal  $\Omega$  from each of the angular rate sensors.

[0015] As shown in FIG. 2, the multiplexer 30 selects the signal  $S^i$ , and the selected signal is periodically sampled by an analog-to-digital converter 32 at a sampling rate  $f_s$  set by a sampling clock generator 33. The values of the samples are received at an input port 34 of a data processor 35. The data processor is interrupted at the sampling rate  $f_s$  to receive the values of the samples from the analog-to-digital converter 32. An amplitude and frequency estimator program 36 controls the data processor 35 to receive a block of the sampled values, and to estimate the amplitude  $A^i$  and the frequency  $f^i$  of the sampled signal  $S^i$ . A health monitoring program 37 controls the data processor 35 to compare the amplitude and frequency estimates to respective predetermined limits to monitor the health of the system. When the estimated amplitude or frequency is found to be outside the bounds of the predetermined limits, the data processor 35 operates a display device 38 to display an error message to an operator (not shown). The health monitoring program 37 then controls the data processor to change a selection signal from an output port 39 so that the analog multiplexer 30 selects a different one of the signals  $S^1, S^2, S^3, \dots, S^n$ .

[0016] In a specific example, the signals  $S^1, S^2, S^3, \dots, S^n$  each have a frequency of about 10 kilohertz, and the sampling rate is 42 kilohertz. The analog-to-digital converter is an Analog Devices part No. AD676 16-bit 100 kSPS sampling ADC which uses a switched-capacitor/charge redistribution architecture to achieve a 10 microsecond total conversion time. The data processor 35 is a Star Semiconductor SPROC programmable digital signal processing (DSP) integrated circuit which is designed for 24-bit arithmetic. In this system, the method of the present invention provides both amplitude and frequency estimates using a modest amount of computation and with errors on the order of parts per million.

[0017] Because the sampling rate  $f_s$  is only about four (sometimes as low as three) times the frequency of the sinusoidal signals  $S^1, S^2, S^3, \dots, S^n$ , the sinusoidal signals are sparsely sampled. The amplitude and frequency estimation method of the present invention, however, provides an accurate estimate of the amplitude and frequency of such a sparsely sampled sinusoidal signal. The method of the present invention can also provide amplitude and frequency estimates based on as few as four samples of a sparsely sampled signal, in the presence of a DC bias.

[0018] Consider first the simplified case of a sinusoid without a DC bias. Assuming that the sinusoid has an amplitude  $A$ , a frequency  $\omega_o$ , and a phase angle  $\phi$ , and assuming that the sampling frequency  $f_s$  has a period  $T=1/f_s$ , then the  $n$ th signal sample  $x_n$  has a value of:

$$x_n = A \sin(\omega_o nT + \phi) \quad (\text{Equation 2})$$

[0019] Since there are three unknowns in Equation 2, it should be possible to extract the amplitude  $A$  and a function of the frequency  $F=\cos\omega_o T$  from three samples of the sinusoidal signal. The two neighboring samples  $x_{n+1}$  and  $x_{n-1}$  are:

$$x_{n+1} = A \sin(\omega_o nT + \phi) \cos(\omega_o T) + A \cos(\omega_o nT + \phi) \sin(\omega_o T) \quad (\text{Equation 3})$$

$$x_{n-1} = A \sin(\omega_o nT + \phi) \cos(\omega_o T) - A \cos(\omega_o nT + \phi) \sin(\omega_o T) \quad (\text{Equation 4})$$

[0020] The function of frequency  $F$  is extracted from the three samples  $x_n, x_{n+1}$  and  $x_{n-1}$  by adding Equations 3 and 4 together, and dividing the sum by Equation 2, to provide:

$$F = \cos\omega_o T = \frac{x_{n+1} + x_{n-1}}{2x_n} \quad (\text{Equation 5})$$

[0021] The amplitude  $A$  is extracted by subtracting the product of Equation 3 and Equation 4 from the square of Equation 2, to provide:

$$x_n^2 - x_{n+1}x_{n-1} = A^2 \sin^2 \omega_o T$$

(Equation 6)

5 [0022] Applying the trigonometric identity  $1 = \cos^2 \alpha + \sin^2 \alpha$  to Equation 5 gives:

$$1 - \left( \frac{x_{n+1} + x_{n-1}}{2x_n} \right)^2 = \sin^2 \omega_o T$$

10 [0023] Dividing Equation 6 by Equation 7 gives:

$$A^2 = \frac{x_n^2 - x_{n+1}x_{n-1}}{1 - \left( \frac{x_{n+1} + x_{n-1}}{2x_n} \right)^2} = \frac{4x_n^2(x_n^2 - x_{n+1}x_{n-1})}{4x_n^2 - (x_{n+1} + x_{n-1})^2}$$

15 [0024] A direct implementation of Equation 8 to solve for the amplitude A therefore requires four multiplies, 3 adds, and 1 divide.

20 [0025] Consider now the more complicated problem of finding the amplitude of a sinusoidal signal superimposed on a DC bias. The signal becomes:

$$y_n = DC + B \sin(\omega_o nT + \phi) \quad (Equation 9)$$

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[0026] Since there are now four unknowns, at least four samples are needed to determine the amplitude B and function of frequency  $F = \cos \omega_o T$ . The DC bias is eliminated by taking the differences  $x_n$  between successive signal samples  $y_n$  and  $y_{n-1}$  as follows:

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$$x_n = y_n - y_{n-1}$$

$$= B[\sin(\omega_o nT + \phi) - \sin(\omega_o (n-1)T + \phi)]$$

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$$= B[\sin(\omega_o nT + \phi) - \sin(\omega_o nT + \phi)\cos \omega_o T + \cos(\omega_o nT + \phi)\sin \omega_o T]$$

$$= B[\sin(\omega_o nT + \phi)(1 - \cos \omega_o T) + \cos(\omega_o nT + \phi)\sin \omega_o T]$$

$$= B\sqrt{2-2\cos \omega_o T} \sin(\omega_o nT + \Theta)$$

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where

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$$\Theta = \phi + \tan^{-1} \left( \frac{\sin \omega_o T}{1 - \cos \omega_o T} \right)$$

(Equation 10)

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[0027] The DC biased sinusoid problem has been transformed to a mathematical form similar to the case without DC bias, except Equation 10 needs to be solved for B. But by comparison:

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$$A = B\sqrt{2-2\cos \omega_o T} \quad (Equation 11)$$

so that:

$$B = \frac{A}{\sqrt{2-2F}}$$

(Equation 12)

5 or:

$$10 B^2 = \frac{A^2}{2-2F} = \frac{2x_n^2}{1-F} \frac{x_n^2 - x_{n+1}x_{n-1}}{(2x_n)^2 - (x_{n+1} + x_{n-1})^2} \quad (\text{Equation 13})$$

Solving Equations 6 and 7 for F gives:

$$15 F = \frac{x_{n+1} + x_{n-1}}{2x_n} \quad (\text{Equation 14})$$

Eliminating F from Equation 14 gives:

$$20 B^2 = \frac{4x_n^3 (x_n^2 - x_{n+1}x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})] [(2x_n)^2 - (x_{n+1} + x_{n-1})^2]} \quad (\text{Equation 15})$$

25 Factoring and re-grouping the terms in the denominator of Equation 15 gives an equivalent expression for the amplitude B:

$$30 B^2 = \frac{4x_n^3 (x_n^2 - x_{n+1}x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]} \quad (\text{Equation 16})$$

35 [0028] Turning now to FIGS. 3, 4, and 5, there is shown a flow graph of a specific procedure implementing Equations 14 and 16 above. This flow graph represents the solution procedure in a form similar to the representation for a digital filter, and indeed the elements in FIGS. 3, 4, and 5 could be individual computational hardware elements. Alternatively, the functions represented by the elements in FIGS. 3, 4, and 5 could be performed by a programmed digital data processor.

40 [0029] As shown in FIG. 3, the sampled signal  $S_i$  is delayed by one sample period T in a register 50 to produce the delayed sample  $S_{i-1}$ . A subtractor 51 subtracts the delayed sample  $S_{i-1}$  from the sample  $S_i$  to produce a difference  $x_i$ . The difference  $x_i$  is delayed by a first sample period T in a second register 52 to provide a delayed difference  $x_{i-1}$ , and is delayed for a second sample period T in a third register 53 to produce a doubly-delayed difference  $x_{i-2}$ .

45 [0030] To compute the denominator of Equation 14, the delayed difference  $x_{i-1}$  is scaled by a factor of two, as represented by a box 54, which could left-shift the delayed difference by one binary place. To produce the numerator (num<sub>i</sub>) of Equation 14, an adder 55 adds the difference  $x_i$  to the doubly-delayed difference  $x_{i-2}$ .

50 [0031] To compute the denominator (DEN<sub>i</sub>) of Equation 16, a subtractor 56 computes the difference (den<sub>i</sub> - num<sub>i</sub>), and an adder 57 computes the sum (den<sub>i</sub> + num<sub>i</sub>). A multiplier 58 squares the difference from the subtractor 56, and a multiplier 59 multiplies the square by the sum from the adder 57 to produce the denominator DEN<sub>i</sub> of Equation 16.

55 [0032] To compute the numerator (NUM<sub>i</sub>) of Equation 16, a multiplier 60 computes the square of the delayed difference  $x_{i-1}$ , and a multiplier 61 computes the cube of the delayed difference  $x_{i-1}$ . A multiplier 62 computes the product of the difference  $x_i$  and the doubly-delayed difference  $x_{i-2}$ . A subtractor 63 computes the difference between the square from the multiplier 60 and the product from the multiplier 62. A multiplier 64 computes the product of the difference from the subtractor 63 and the cube from the multiplier 61. The product from the multiplier 64 is scaled by a factor of four as indicated in a box 65, which could represent a left-shift by two binary places, to produce the numerator NUM<sub>i</sub> of Equation 16.

[0033] A divider 66 computes the quotient F<sub>i</sub> of Equation 13, and a divider 67 computes the quotient B<sub>i</sub><sup>2</sup> of Equation 15. The division performed by the divider units 66, 67 preferably is a polynomial approximation as derived in Appendix I.

[0034] Continuing now in FIG. 4, the values of B<sub>i</sub><sup>2</sup> are filtered in a digital filter 81 to determine average values  $\bar{B}_i^2$ . The digital filter 81, for example, is a non-recursive digital filter including a shift register storing the values B<sub>i-1</sub><sup>2</sup>, B<sub>i-2</sub><sup>2</sup>,

and  $B_{i-3}^2$  and computing the sum of  $B_i^2$  and these three values and dividing the sum by four, by a right-shift by two binary places, to provide a ~~average~~ average value  $\bar{B}_i^2$ . The square root of this average value is computed by a computational unit 82. The computational unit 82, for example, performs a square root operation by a polynomial approximation as derived in Appendix II. The result of the square root operation is an estimate  $B_i$  of the amplitude of the sampled sinusoidal signal S.

[0035] The division operation performed by the divider 76 in FIG. 3 may give an inaccurate result when the value of the denominator  $DEN_i$  is approximately zero. To prevent such inaccurate results from corrupting the amplitude estimate  $B_i$ , the inaccurate values of  $B_i^2$  can be excluded so as not to be averaged by the digital filter 81. For this purpose, a digital multiplexer 83 selects either the value  $B_i^2$  from the division unit 67 in FIG. 3, or selects the previous average value computed by the digital filter 81. The previous average value computed by the digital filter 81 is obtained from a register 84, that is clocked at the sampling frequency  $f_s$ . To determine when the value  $B_i^2$  may be erroneous, the value  $DEN_i$  of the divisor for the division unit 67 is received by an absolute value unit 85 that determines the magnitude of the divisor value  $DEN_i$ . A comparator 86 compares this magnitude to a certain fraction of the average value of the divisor value. A digital filter 87, which may be similar to the digital filter 81, computes the average of the divisor value, and a shifter 88 right-shifts the average divisor value by N binary places to compute a predetermined fraction of the average of the divisor value. The value of N, for example, is three.

[0036] Turning now to FIG. 5, it is seen that the quotient  $F_i$  of Equation 13 is processed in a similar fashion to the processing of the quotient  $B_i^2$  as shown in FIG. 4, by a digital filter 91, a functional unit 92, a multiplexer 93, a register 94, an absolute value unit 95, a comparator 96, a digital filter 97, and a right-shifter 98, that are similar to the corresponding components 81 to 87 in FIG. 4. The functional unit 92 in FIG. 5, however, computes an arc-cosine function  $(1/2\pi T)\arccos(\bar{f}_i)$ . The functional unit 92 preferably computes this arc-cosine function as a polynomial approximation, as derived in Appendix III.

[0037] In practice, the estimates of amplitude  $B_i$  and frequency  $f_i$  are relatively correlated between the neighboring  $i^{\text{th}}$  and  $i+1^{\text{th}}$  values. Therefore, it is possible to reduce the computational requirements of obtaining an estimate with only a slight decrease in performance by computing an amplitude estimate  $B$  and frequency estimate  $f$  from non-overlapping triplets of differences, rather than by computing the estimates from overlapping triplets of differences as illustrated in FIGs. 3, 4, and 5. In other words, although the computations illustrated in FIGs. 3, 4, and 5 can provide the best performance and provide a new estimate of the amplitude  $B_i$  and  $f_i$  at each sampling instant, the computational requirements for computing such estimates at each sampling instant are rather burdensome because all of the computations shown in FIGS. 3, 4, and 5 must be performed over each sampling period T. For monitoring the health of signals in a system as illustrated in FIG. 2, for example, it is not necessary to compute a new estimate of amplitude or frequency for each sampling instant. Therefore, the computational requirements for monitoring the health of signals in a system as shown in FIG. 2 can be considerably relaxed by performing the computations illustrated in FIG. 3 over non-overlapping triplets of differences, and by performing the digital filtering and square root or arc-cosine function from the ratios computed from a number of non-overlapping triplets of differences.

[0038] Turning now to FIG. 6, there is shown a flow diagram for the computations that are preferably performed for the system of FIG. 2 in the data processor 35. As illustrated in FIG. 6, an amplitude estimate  $B$  and a frequency estimate  $f$  are obtained from 16 non-overlapping triplets of differences  $x_1, x_2, x_3; x_4, x_5, x_6; x_7, x_8, x_9; \dots; x_{46}, x_{47}, x_{48}$ . The triplets of differences are the results of difference computations 101, 102, 103, ... 104, that are preferably performed by an interrupt program when the data processor 35 of FIG. 2 is interrupted at the sampling frequency  $f_s$ . A quotient  $B_i^2$  and  $F_i$  for each of the triplets of differences are computed by ratio computations 105, 106, 107 ... 108 that are performed at a rate of one-third of the sampling frequency  $f_s$ . The 16 quotients  $B_i^2$  and the 16 quotients  $F_i$  are accumulated in digital filtering 109 that can be performed at various times over about 48 sampling periods T corresponding to the differences  $x_i$  to  $x_{48}$ . The average values of the quotient  $B^2$  and  $\bar{F}$  result from the digital filtering. A square root function 110 computes the amplitude estimate  $B$  from the average value of the quotient  $B^2$ , and the frequency estimate  $f$  is computed by an arc-cosine function 111 from the average value of the quotient  $\bar{F}$ .

[0039] Also shown in FIG. 6 is a variable Q associated with the amplitude estimate  $B$ , and a variable q associated with the frequency estimate  $f$ . The variables Q and q indicate, respectively, the number of the quotient values  $B_i^2$  and  $F_i$  that were actually averaged together by the digital filter 109 instead of being excluded because their associated denominator value  $DEN_i$  or  $den_i$ , respectively, was relatively small. In contrast to FIGs. 4 and 5, where the exclusion condition was a certain fraction of an average value of  $DEN_i$  or  $den_i$ , respectively, the digital filter 109 preferably rejects quotients when the value of  $DEN$  or  $den$  falls below a respective predetermined threshold value. In the system of FIG. 3, for example, the amplitude estimate  $B$  or the frequency estimate  $f$  should fall within certain predetermined limits, so that the threshold can be set at a certain fraction of the average value expected for any healthy signal. The threshold value is not critical and can be determined by simple trial and error for a particular system.

[0040] Listed below is an example program that performs the functions shown in FIG. 6 and which corresponds to the amplitude and frequency estimator program 36 and the health monitoring program 37 of FIG. 2. In particular, in the listing below, there is shown a main program called "MONITOR" that operates the analog multiplexer 30 of FIG. 2

to scan among three signals. Upon outputting a new select signal to the multiplexer, the program MONITOR waits 30 microseconds for the analog-to-digital converter 32 to sample the new signal. Then the program MONITOR calls a routine called TESTSIG in order to test whether the amplitude and frequency of the selected signal are within predetermined limits. If not, the program MONITOR displays an error code provided by the TESTSIG routine, and then the program MONITOR selects another signal for processing.

[0041] The TESTSIG routine initializes a number of variables used by a 42 kHz interrupt routine corresponding to the amplitude and frequency estimator program 36 of FIG. 2. After initializing these variables, the TESTSIG routine enables a 42 kHz interrupt so that the amplitude and frequency estimator program processes the signal samples from the analog-to-digital converter 32 in FIG. 2. The routine TESTSIG polls a variable NUMC to determine when the amplitude and frequency estimator program 36 is finished. When NUMC is greater or equal to 16, then the amplitude and frequency estimator program 36 is finished. The TESTSIG routine then compares the variables Q and q to predetermined minimum limits QMIN and qmin, and also compares the amplitude estimate B and the frequency estimate f to respective predetermined minimum and maximum limits. An error indication is produced when any one of the variables Q, q, B, or f is outside of a boundary set by a respective one of the limits.

[0042] The 42 kHz interrupt routine inputs one sample during each interrupt and classifies the sample as either case0, case1, case2, or case3. Case0 corresponds to the very first sample S1, and the other three cases correspond to one of the samples that permits the computation of either a first difference, a second difference, or a third difference, respectively, for each of the 16 triplets of differences. When a triplet of differences has been accumulated, then the computations depicted in FIG. 3 are performed for the triplet to compute a quotient  $B_i^2$  and  $F_i$  for the triplet. Also included in the program listing are examples of functions for computing the ratios, the square roots, and the arc-cosines by the polynomial approximations as derived in Appendices I, II, and III.

```

MONITOR  SELECT ← SELECT +1
25        IF SELECT > 3 THEN SELECT ← 1
          OUTPUT SELECT
          WAIT 30 MICROSECONDS
          CALL TESTSIG
          IF ERROR > 0 THEN GOTO 10
          B (SELECT) ← SQRT(BS)
30        *** NOTE:   K = 1/2πT
          f (SELECT) ← K*ACOS(F)
          RETURN
10        DISPLAY(ERROR)
          RETURN
35        TESTSIG  ERROR ← 0
          CASE ← 0
          NUMC ← 0
          BS ← 0
          F ← 0
40        Q ← 0
          q ← 0
          ENABLE 42 kHz INTERRUPT
110       IF NUMC < 16 THEN GOTO 110 IF Q ≥ QMIN THEN GOTO 120 ERROR ← 1
          RETURN
45        120     BS ← BS/Q
          IF BS ≤ BSMAX THEN GOTO 130 ERROR ← 2
          RETURN
130       IF BS ≥ BSMIN THEN GOTO 140 ERROR ← 3
          RETURN
50        140     IF q ≥ qmin THEN GOTO 150
          ERROR ← 4
          RETURN
150       F ← F/q
          F ≤ FMAX THEN GOTO 160 ERROR ← 5
          RETURN
55        160     IF F ≥ FMIN THEN RETURN ERROR ← 6
          RETURN
42KHZINT INPUT SAMPLE

```

```

        IF CASE > 0    THEN GOTO 210 S1 ← SAMPLE
        CASE ← 1
        RETURN
210      IF CASE > 1    THEN GOTO 220 X1 ← S1 - SAMPLE
5        S1 ← SAMPLE
        CASE ← 2
        RETURN
220      IF CASE > 2    THEN GOTO 230 X2 ← S1 - SAMPLE
10      S1 ← SAMPLE
        CASE ← 3
        RETURN
230      X3 ← S1 - SAMPLE
        S1 ← SAMPLE
        CASE ← 1
15        num ← X1 + X3
        PRODX1X3 ← X1 * X3
        NUMC ← NUMC + 1
        IF NUMC ≥ 16    THEN GOTO 240 CLEAR INTERRUPT MASK
        GOTO 250
20      240      DISABLE 42 KHZ INTERRUPT
250      SQX2 ← X2 * X2
        CUBX2 ← SQX2*X2
        den ← LEFT SHIFT X2 BY 1
        SUMnd ← num + den
25      DEN ← den - num
        DEN ← DEN*DEN
        DEN ← DEN*SUMnd
        NUM ← SQX2 - PRODX1X3
        NUM ← NUM*CUBX2
30      LEFT SHIFT NUM BY 2
        IF den < denmin    THEN GOTO 260
        F ← F + RATIO(num,den)
        q ← q + 1
260      260      IF DEN < DENMIN    THEN GOTO 270
35      BS ← BS + RATIO(NUM,DEN)
        Q ← Q + 1
270      RETURN

40      FUNCTION RATIO (T/U)
        *** NOTE:
        *** B0 = 0.8946079612
        *** B1 = -0.3153155446
        *** B2 = 0.0547355413
        *** B3 = -0.0046808124
45      *** B4 = 0.0001578331
        RATIO ← U*B4
        RATIO ← RATIO + B3
        RATIO ← RATIO * U
        RATIO ← RATIO + B2
50      RATIO ← RATIO * U
        RATIO ← RATIO + B1
        RATIO ← RATIO * U
        RATIO ← RATIO + B0
        RATIO ← RATIO * T
55      RETURN

        FUNCTION SQRT(V)
        *** NOTE:

```

```

*** A0 = 0.5439969897
*** A1 = 0.5490743
*** A2 = -0.0689262746
*** A3 = 0.0068873167
5 *** A4 = -0.0003057122
      SQRT ← V * B4
      SQRT ← SQRT + B3
      SQRT ← SQRT * V
      SQRT ← SQRT + B2
10     SQRT ← SQRT * V
      SQRT ← SQRT + B1
      SQRT ← SQRT * V
      SQRT ← SQRT + B0
      /
      RETURN

15     FUNCTION ACOS(w)
      *** NOTE:
      *** C0 = 0.0500000119
      *** C1 = -0.6684602499
20     *** C2 = -0.1108554006
      *** C3 = -0.0580515265
      SQW ← W * W
      ACOS ← SQW * C3
      ACOS ← ACOS + C2
25     ACOS ← ACOS * SQW
      ACOS ← ACOS + C1
      ACOS ← ACOS * W
      ACOS ← ACOS + C0
      RETURN

```

30 [0043] Finally, shown in Appendix IV is a computer program for evaluating the performance of various embodiments of the present invention.

35 [0044] In view of the above, there has been described a method for estimating the amplitude and phase of a biased and sparsely-sampled sinusoidal signal. The method can give accurate results from a small number of samples, with only a modest amount of computation. Therefore, the method is easily implemented by a data processor programmed for estimating the amplitude and frequency of a number of analog signals scanned by an analog multiplexer and digitized by an analog-to-digital converter.

40

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## PERFORMANCE EVALUATION

5

$$AF := \left[ \sum_p b_p y_p \right] \quad \text{The approximating function.}$$

10

$$ERROR := REF - AF \quad \text{The performance error.}$$

The plot of the error-extremal envelope bounded by  $\epsilon'$ :

15

$$\epsilon' := \text{if } [\epsilon = 0, \max [|ERROR|], |\epsilon|] \quad \text{Another index } i := 0 \dots 1$$

20

This is the error-extremal envelope plot:

$$EY_k := \text{if } [k = K - 1, 0, \text{if } [ERROR_{k+1} \geq ERROR_k, \epsilon', -\epsilon'] ]$$

25

This filter (MASK) is used to locate the frequencies corresponding to all extremal error values plus the end points:

$$MASK_k := \text{if } [k = 0, 1, \text{if } [k = K - 1, 1, \text{if } [EY_{k+1} = -EY_k, 1, 0] ] ]$$

30

This is the actual frequency-filtering operation. The only frequencies that get through are the end points plus those where error extrema are located.

35

$$MATRIX_{k,0} := y_k \cdot MASK_k$$

$$MATRIX_{k,1} := |ERROR_k| \cdot MASK_k$$

40

Extract the frequencies where the  $N+1$  largest end-point values and extremal values are located, sort them, and write them into memory:

45

$$MYE_{n,i} := \text{reverse}(\text{csort}(MATRIX, 1))_{n,i} \quad SYE := (\text{csort}(MYE, 0))$$

50

$$|\epsilon| = 5.42 \cdot 10^{-5}$$

$$\text{WRITERPN}(YA) := SYE^{<0>}$$

55

$$\max [(\text{ERROR})] - \epsilon = 1.25 \cdot 10^{-5}$$

5 A sanity check.

$$10 \text{floor} \left[ \frac{-\log [\max [(\text{ERROR})]]}{\log (2)} \right] = 13$$

Accuracy performance level  
measured in bits.  
Compute the peak error in  
ppm

15 Now plot the functions and the  
error

$$\max [(\text{ERROR})] \cdot 10^6 = 66.7$$

20 List the extremal frequencies  
(col 0), and the extremal value  
magnitudes (col 1):

The rounded coefficients:

$$25 SYE = \begin{bmatrix} 4 & 0.0000522733 \\ 4.3283283283 & 0.0000564838 \\ 5.2452452452 & 0.0000502018 \\ 6.5025025025 & 0.0000612455 \\ 7.5635635636 & 0.0000433821 \\ 8 & 0.0000666976 \end{bmatrix}$$

$$b = \begin{bmatrix} 0.8946079612 \\ -0.3153155446 \\ 0.0547355413 \\ -0.0046808124 \\ 0.0001578331 \end{bmatrix}$$

25 The hex coefficients:

$$30 \frac{\max [(\text{SYE}^{<1>})]}{\min [(\text{SYE}^{<1>})]} - 1 = 0.5374449341$$

$$2^8 \cdot b = \begin{bmatrix} e50507h \\ -50b885h \\ e0326h \\ -132c3h \\ a58h \end{bmatrix}$$

40 END OF PROGRAM

45 CHEBYCHEV APPROXIMATION FOR SQUARE ROOT USING THE REMEZ-EXCHANGE ALGORITHM QRSSQRT.  
MCD

[0045] The objective of this program is to calculate the "a" coefficients that provide a Chebychev polynomial approximation to the square root of y.

[0046] The Chebychev solution is the one that minimizes the maximum error of the approximation fit. There are no "surprise points" in the solution space.

50

55

5

## INITIALIZE

Y<sub>nom</sub> := 2

Nominal value of the output variable.

10

δY := 0.1·Y<sub>nom</sub>

Tolerance on the output variable.

15

X<sub>max</sub> := [Y<sub>nom</sub> + δY]<sup>2</sup>X<sub>max</sub> = 4.84 Maximum anticipated input value

20

X<sub>min</sub> := [Y<sub>nom</sub> - δY]<sup>2</sup>X<sub>min</sub> = 3.24 Minimum anticipated input value

25

B := 24

Number of bits of coefficients resolution.

N := 5

Number of coefficients in data-fitting routine. (This is determined by trial and error.).

30

n := 0 .. N

Coefficient index.

m := 0 .. N

The y-value index.

p := 0 .. N - 1

The weighting-coefficient ("b") index.

35

K := 1000

Number of performance-evaluation points.

k := 0 .. K - 1

Performance-evaluation index.

40

PRINTCOLWIDTH := 10

PRNPRECISION := 10

ZERO := 0

WRITERPN(XA) := ZERO □

m

WRITE(COUNT) := 0 □

TYPE "PROCESS", COMMENT "WRITERPN(XA)" &amp; "WRITE(COUNT)". THEN GOTO 128.

45

50

55

## SETUP

5      ITERATION := READ(COUNT)    WRITE(COUNT) := 1 + ITERATION    XA :=  
 READPRN (XA)

10       $X_N := \text{if } [ITERATION = 0, X_{\min} + [X_{\max} - X_{\min}] \cdot \frac{m}{n}, X_{\max}]$

The extreme values of the independent variable.

15       $M_{m,n} := \text{if } [n = N, (-1)^m, X_m^m]$

The Remez matrix.

20       $x_k := X_{\min} + [X_{\max} - X_{\min}] \cdot \frac{k}{K - 1}$

The performance-evaluation variable.

25       $R := [\sqrt{X}] \quad REF := [\sqrt{X}]$

R is the functional reference vector; REF is the performance-reference vector.

30       $v := M^{-1} \cdot R \quad \epsilon := v_N$

v is the solution vector;  $\epsilon$  is the error measure

35       $a_p := 2^{-B} \cdot \text{floor} [0.5 + 2^B \cdot v_p]$

The coefficient vector rounded to B bits.  
 WRITEPRN(ACOEFF) := a

\*\*\*\*\*  
PERFORMANCE EVALUATION

40       $AF := \left[ \sum_p a_p \cdot x^p \right]$

The approximating function.

45      ERROR := REF - AF

The performance error.

The plot of the error-extremal envelope bounded by  $\epsilon$ :

50

55

$\epsilon' := \text{if } [\epsilon \approx 0, \text{max}(|\text{ERROR}|), |\epsilon|]$

Another index:  $i := 0 \dots 1$

5

This is the error-extremal envelope plot:

$EX_k := \text{if } [k = K - 1, 0 \text{ if } [\text{ERROR}_{k+1} \geq \text{ERROR}_k, \epsilon', -\epsilon']]$

This filter (MASK) is used to locate the frequencies corresponding to all extremal error values, plus the end points:

$\text{MASK}_k := \text{if } [k = 0, 1, \text{if } [k = K - 1, 1, \text{if } [\text{EX}_{k+1} = -\text{EX}_k, 1, 0]]]$

20 This is the actual frequency-filtering operation. The only frequencies that get through are the end points plus those where extremal are located.

$$\text{MATRIX}_{k,0} := x_k \cdot \text{MASK}_k \quad \text{MATRIX}_{k,1} := \text{ERROR}_k \cdot \text{MASK}_k$$

25

Extract the frequencies where the  $N+1$  largest end-point values and extremal values are located, sort them, and write them into memory.

**MXE** := reverse (csort(MATRIX\_1)) . . . SXE := (csort(MXE\_1))

-6

103

35 |ε| = 1.1 10 WRITEPRN(XA) := SXE

40  $\max \left[ \left| \text{ERROR} \right| \right] = |\epsilon| = 3.41 \cdot 10^{-7}$  A sanity check.

$$45 \quad \text{floor} \left[ \frac{-\log(\max(|\text{ERROR}|))}{\log(2)} \right] = 19$$

Accuracy performance level measured in bits.

50

55

Now plot the functions and the error

Compute the peak error in ppm:

5

$$\max(|\text{ERROR}|) \cdot 10^6 = 1.44$$

10 List the extremal frequencies (col 0), and the extremal values (col 1):

The rounded coefficients are:

15

$$\text{SXE} = \begin{vmatrix} 3.24 & 0.0000010195 \\ 3.384144141 & 0.0000011859 \\ 3.7669269269 & 0.0000009604 \\ 4.2682282282 & 0.0000013106 \\ 4.675035035 & 0.0000007948 \\ 4.84 & 0.0000014362 \end{vmatrix}$$

$$a = \begin{vmatrix} 0.5439969897 \\ 0.5490743518 \\ -0.0689262748 \\ 0.0068873167 \\ -0.0003057122 \end{vmatrix}$$

20

25

$$\frac{\max(|\text{SXE}^{(1)}|)}{\min(|\text{SXE}^{(1)}|)} - 1 = 0.8069951557$$

The hex coefficients:

$$2^8 \cdot a = \begin{vmatrix} 8b4363h \\ 8c9023h \\ -11a527h \\ 1c35eh \\ -1409h \end{vmatrix}$$

30

END OF PROGRAM

35

APPENDIX III.

MATHCAD (Trademark) PROGRAM CHEBYCHEV APPROXIMATION TO AN ARCCOSINE FUNCTION  
QRSARCOSRMZ.MCD

40

[0047] The objective of this program is to calculate the "a" coefficients that provide the Chebychev solution to the polynomial approximation of  $\arccos(x)$ . The application is a direct-reading frequency-deviation meter. We are going to estimate  $\delta f/f_0$ .

45

50

55

## INITIALIZE

5	$f_s := 42000$	The sampling frequency.
	$f_0 := 10000$	The nominal frequency.
	$\delta f := 0.2 \cdot f_0$	Maximum deviation of the variable to be estimated.
10	$Y_{\max} := \cos \left[ [f_0 - \delta f] \cdot \frac{2\pi}{f_s} \right]$	Maximum value of the input variable $Y_{\max} = 0.3653410244$ .
15	$Y_{\min} := \cos \left[ [f_0 + \delta f] \cdot \frac{2\pi}{f_s} \right]$	Minimum value of the input variable $Y_{\min} = 0.222520934$ .
20	$B := 24$	Number of bits of coefficient resolution.
25	$N := 4$	Number of coefficients in data-fitting routine.
	$n := 0 .. N$	Coefficient index.
	$m := 0 .. N$	The x-value index.
30	$p := 0 .. N - 1$	The weighting-coefficient ("a") index.
	$K := 1000$	Number of performance-evaluation points.
35	$k := 0 .. K - 1$	Performance-evaluation index.
	$PRINTCOLWIDTH := 10$	
	$ZERO := 0$	$PRNPRECISION := 10$
	$m$	$WRITEPRN(YA) := ZERO$
40	TYPE "PROCESS", COMMENT "WRITEPRN(YA)" & "WRITE(COUNT)". THEN "GOTO 140".	$WRITE(COUNT) := 0$
	*****	
45		
50		

## SETUP

5    ITERATION := READ(COUNT)    WRITE(COUNT) := 1 + ITERATION  
 YA := READPRN(YA)

10     $Y_m := \text{if } [ITERATION = 0, Y_{\min} + [Y_{\max} - Y_{\min}] \cdot \frac{m}{N}, YA_m]$

15    The extremal values of the  
 independent variable, y.

15     $M_{m,n} := \text{if } [n = N, (-1)^m, \text{if } [n = 0, 1, Y_m^{2 \cdot n - 1}]]$

20    The Remez matrix.

25     $y_k := Y_{\min} + [Y_{\max} - Y_{\min}] \cdot \frac{k}{K - 1}$     The performance-evaluation  
 variable.

30     $R := \frac{f_s}{2\pi \cdot f_o} \cdot \overline{\cos(Y)} - 1$     R is the functional reference  
 vector; REF is the  
 performance-reference vector.

35     $REF := \frac{f_s}{2\pi \cdot f_o} \cdot \overline{\cos(y)} - 1$

40     $v := M^{-1} \cdot R$      $\epsilon := v_N$     v is the solution vector;  $\epsilon$  is  
 the error measure.

45     $a_p := 2^{-B} \cdot \text{floor} [0.5 + 2^B \cdot v_p]$     The coefficient vector rounded  
 to B bits.  
 WRITEPRN(CCOEFF) := a

50

55

## PERFORMANCE EVALUATION

5       $b_p := \text{if } [p = 0, 0, a_p]$

10      $AF := a_0 + \left[ \sum_p b_p y^{2p-1} \right]$       The approximating function.

15     ERROR := REF - AF      The performance error.

The plot of the error-extremal envelope bounded by  $\epsilon'$ :

20      $\epsilon' := \text{if } [\epsilon = 0, \max [(|\text{ERROR}|), |\epsilon|]]$       Another index:  $i := 0 \dots 1$

25      $EY_k := \text{if } [k = K - 1, 0, \text{if } [\text{ERROR}_{k+1} \geq \text{ERROR}_k; \epsilon', -\epsilon']]$

This filter (MASK) is used to locate the frequencies corresponding to all extremal error values:

30      $\text{MASK}_k := \text{if } [k = 0, 1, \text{if } [k = K - 1, 1, \text{if } [EY_{k+1} = -EY_k, 1, 0]]]$

35     This is the actual filtering operation. The only frequencies that get through are those where error extrema are located.

40      $\text{MATRIX}_{k,0} := Y_k \cdot \text{MASK}_k$        $\text{MATRIX}_{k,1} := |\text{ERROR}_k| \cdot \text{MASK}_k$   
Extract the frequencies where the  $N+1$  largest extremal values are located, sort them, write them into memory, and list the rounded coefficients:

45      $\text{MYE}_{m,i} := \text{reverse}(\text{csort}(\text{MATRIX}, 1))_{m,i}$        $\text{SYE} := (\text{csort}(\text{MYE}, 0))$

50

55

$$|\epsilon| = 5.02 \cdot 10^{-7}$$

$$5 \quad \max [(\text{ERROR})] - |\epsilon| = 1.58 \cdot 10^{-8}$$

WRITERPRN(YA) := SYE<sup><0></sup>

"Gut" insurance. (If you can't feel good about the solution, its probably wrong!)

$$10 \quad \text{floor} \left[ \frac{-\log [\max [(\text{ERROR})]]}{\log (2)} \right] = 20$$

Accuracy performance level measured in bits.

15 Now plot the functions and the error

$$\max [(\text{ERROR})] = 5.18 \cdot 10^{-7}$$

20 The extremal values:

$$25 \quad SYE = \begin{vmatrix} -0.0830581871 & 0.0000005136 \\ 0.0817079274 & 0.0000004898 \\ 0.2294089799 & 0.0000005165 \\ 0.3294455494 & 0.0000004871 \\ 0.3653410244 & 0.0000005183 \end{vmatrix}$$

The rounded coefficients:

$$a = \begin{vmatrix} 0.0500000119 \\ -0.6684602499 \\ 0.1108554006 \\ -0.0580515265 \end{vmatrix}$$

$$30 \quad \frac{\max [(\text{SYE}^{<1>})]}{\min [(\text{SYE}^{<1>})]} - 1 = 0.0639659227$$

$$2^3 \cdot a = \begin{vmatrix} cccccdh \\ -ab2036h \\ -1c6105h \\ -edc77h \end{vmatrix}$$

35

END OF PROGRAM

40

45

50

55

#### APPENDIX IV.

MATHCAD (Trademark) PROGRAM  
SIMPLE AND ROBUST QRS DRIVE-VOLTAGE  
AMPLITUDE AND FREQUENCY ESTIMATION  
QRSSINEAMPLY.MCD

## SUMMARY

This program introduces an algorithm that computes the peak amplitude of the sparsely sampled noisy sinusoid riding on a dc offset. The algorithm uses only adds, multiplies, and shifts operating on sets of 4 contiguous samples. The inherent computational error is on the order of 15 ppm. The algorithm also estimates frequency; the inherent computational error is within 2 or 3 hundredths of a Hertz. Naturally, high noise levels degrade the performance.

## SETUP AND DEFINITIONS

$K := 128$	$k := 0 .. K - 1$	Source-signal index
$L := K - 1$	$l := 0 .. L - 1$	Processed-signal index
$M := L - 2$	$m := 0 .. M - 1$	Signal-processing index
.	$n := 0 .. M - 1$	... and another one.
$f_s := 42000$		Sampling frequency
$T := \frac{1}{f_s}$	$T = 2.381 \cdot 10^{-5}$	Sampling period
$A_0 := 2$		$A$ is the signal amplitude (the nominal value is $A_0$ we allow $+/- 10\%$ variation)
$A := A_0 \cdot (1 + (-0.1 + \text{rnd}(0.2)))$	$A = 1.937$	
$f_0 := 10000$		Nominal signal frequency
$f' := f_0 \cdot (1 + 0.2 \cdot (\text{rnd}(2) - 1))$		Signal frequency (Hz). $+/- 20\%$ variation is allowed about the nominal.

$\Omega := 2 \cdot \pi \cdot f'$ , Signal frequency  
(rad/sec)  
 5  $\phi := \text{rnd}(2 \cdot \pi)$   $\phi = 5.266$  A completely arbitrary  
phase angle.  
 10  $u_k := A \cdot \sin(\Omega \cdot T \cdot k + \phi)$  QRS voltage sinusoidal-  
signal samples.  
 15  $\eta_k := 2 \cdot 10^{-3} \cdot (\text{rnd}(2) - 1)$  Now we generate some  
noise ...  
 20  $DC := -1 + \text{rnd}(2)$   $DC = -0.421$  ... and a DC offset  
(arbitrary) ...  
 25  $v := u + \eta + DC$  ... and add them to the  
signal in order to obtain  
the noisy and biased  
input voltage, v.  
 30  $SNR := 10 \cdot \log \left[ \frac{K}{2} \cdot \frac{A^2}{\sum_k \eta_k^2} \right]$  Signal-to-noise ratio (in  
dB) at the input: SNR =  
61.

---

 DEFINE SOME FUNCTIONAL APPROXIMATIONS

35 We use Chebychev (minimax solutions) polynomial approximations to  
 the square root, division, and arccosine operations. The  
 polynomial coefficients have been rounded to 24 bits. These  
 coefficients are imported from the SQRT.MCD, DIVIDE.MCD, and  
 ARCCOSRMZ.MCD programs.

40  $a := \text{READPRN}(ACOEFF)$   $b := \text{READPRN}(BCOEFF)$   $i := 0 \dots \text{last}(a)$   
 $a = \begin{bmatrix} 0.5439969897 \\ 0.5490743518 \\ -0.0689262748 \\ 0.0068873167 \\ -0.0003057122 \end{bmatrix}$   $b = \begin{bmatrix} 0.8946079612 \\ -0.3153155446 \\ 0.0547355413 \\ -0.0046808124 \\ 0.0001578331 \end{bmatrix}$

45  $\text{sqrt}(x) := \sum_i a_i x^i$   
 $\text{sgn}(y) := \text{if}(y \geq 0, 1, -1)$

50

5  $div(x, y) := s \cdot \dots \cdot x \cdot 2$

$$2\text{-}floor\left[\frac{\log(|y|)}{\log(2)}\right] \cdot \sum_i b_i \cdot [|y| \cdot 2^{2\text{-}floor\left[\frac{\log(|y|)}{\log(2)}\right]}]^i$$

10

e.g.,  $div(12, 3) = 4.001$   
 $\sqrt{4} = 2 \quad \sqrt{div(12, 3)} = 2$

15  $nfd = \text{normalized frequency deviation.}$

C := READPRN(CCOEFF)

$$20 C = \begin{bmatrix} 0.0500000119 \\ -0.6684602499 \\ -0.1108554006 \\ -0.0580515266 \end{bmatrix} \quad \text{Example:} \quad nfd[\cos[2\pi f_o \cdot (1 + 0.1) \cdot T]] = 0.100001$$

\*\*\*\*\*

25

### THE PROCEDURE

Our first step is to eliminate the DC offset by taking the difference between successive samples of the input signal. The input signal to the differencing operator is v, the signal after the differencing operator is x:

30  $x_1 := v_{1+1} - v_1 \quad \text{The difference signal}$

35 The estimates of A and frequency are  $EOA := \sqrt{\frac{NUM}{DEN}} \quad Eof := \frac{1}{2\pi \cdot T} \cdot a$

Define:

40  $NUM_m := 4 \cdot x_{m+1}^3 \cdot [x_{m+1}^2 - x_m \cdot x_{m+2}]$

45  $DEN_m := [2 \cdot x_{m+1}]^2 - [x_m + x_{m+2}]^2 \cdot [2 \cdot x_{m+1} - [x_m + x_{m+2}]]$

$num_m := x_{m+2} + x_m \quad den_m := 2 \cdot x_{m+1}$

50

55

5 In order to avoid division problems that arise if the denominators are too small, we define the "weeding-out" functions, p and q:

$$p_m := \text{if } [ |DEN_m| < 0.01 \cdot \max [ (|DEN|), 0, 1 ] ]$$

$$10 q_m := \text{if } [ |den_m| < 0.01 \cdot \max [ (|den|), 0, 1 ] ]$$

15 Now we compute the estimate of the square of A over several sets of samples, average those results, then take the square root:

$$20 EoA := \sqrt{\frac{p}{\sum p} \cdot [ \text{div}(NUM, DEN) ]}$$

and compute the amplitude-estimation error in ppm:

$$25 \epsilon := \frac{|A - EoA|}{A} \cdot 10^6 \quad \epsilon = 16.662$$

30 We similarly estimate the frequency (the actual value is  $f_o$ )

$$35 Eof := f_o \cdot \left[ 1 + nfd \left[ \frac{q}{\sum q} \cdot \text{div}(num, den) \right] \right]$$

$$Eof = 9937.361 \\ f_o = 9937.135$$

40 and determine the frequency-estimation error in Hertz:

$$\epsilon f := f' - Eof \quad \epsilon f = -0.226$$

45 We have been operating with a signal-to-noise ratio of SNR = 61.445 the phase angle is  $\phi = 5.266$  the DC offset is DC = -0.421 the frequency is off nominal by  $f' - f = -62.865$  and the 50 amplitude is off by  $A - A_o = -0.063$  o o.

END OF PROGRAM

55 Claims

1. A method of obtaining and using an indication of a characteristic of sinusoidal signal exciting an angular rate sensor, said method comprising the steps of:

5           a) exciting said angular rate sensor with said sinusoidal signal;  
 b) digitizing said sinusoidal signal in an analog-to-digital converter, thereby producing a sequence of sample values S1, S2, S3...Sn at respective spaced instants of time;  
 c) computing in a computer operating pursuant to software a series of ratios of algebraic functions of triplets xi, xi-1, xi-2 of neighboring ones of said sample values;  
 d) computing in a computer operating pursuant to software an average of said ratios to produce said indication of said characteristic;  
 e) applying said indication of said characteristic to a correction signal generator to produce a correction signal; and  
 10           f) subtracting, in an adder unit, the correction signal from an angular rate signal generated by said angular rate sensor to produce a corrected angular rate signal.

2. The method as claimed in claim 1, wherein:

15           - the indication of the characteristic is an estimate (B) of the amplitude;  
 - the signal is a sinusoidal signal represented as sample values S1, S2, S3, S4 at respective spaced instants of time;  
 - the number of sample values is four; and  
 20           - x1 is the difference between S2 and S1, x2 is the difference between S3 and S2, and x3 is the difference between S4 and S3.

3. The method as claimed in claim 2, wherein said step of computing an estimate (B) of said amplitude is performed by

25           i) computing a ratio of algebraic functions of said triplet of differences x1, x2, and x3 ; and  
 ii) computing said estimate (B) of said amplitude as a nonlinear function of said ratio of algebraic functions.

4. The method as claimed in claim 3, wherein said ratio of algebraic functions includes terms equivalent to:

$$30 \quad \frac{x_n^3(x_n^2 - x_{n+1}x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}.$$

5. The method as claimed in claim 4, wherein said nonlinear function includes a polynomial approximation of a square root function.  
 35  
 6. The method as claimed in claim 2, wherein each of said steps a) and b) are performed by a data processor under program control.  
 40  
 7. The method as claimed in claim 2, further comprising the step of computing a correction value from said estimate (B) of the amplitude of said sinusoidal signal for compensating a parasitic capacitance in an electrical circuit.

8. The method as claimed in claim 1, wherein:

45           - the indication of the characteristic is an estimate (F) of the frequency;  
 - the signal is a sinusoidal signal represented as sample values S1, S2, S3, S4 at respective spaced instants of time;  
 - the number of sample values is four; and  
 50           - x1 is the difference between S2 and S1, x2 is the difference between S3 and S2, and x3 is the difference between S4 and S3.

55           9. The method as claimed in claim 8, wherein said step of computing an estimate (F) of said frequency is performed by  
 i) computing a ratio of algebraic functions of said differences x1, x2, and x3 ; and  
 ii) computing said estimate (F) of said frequency as a nonlinear function of said ratio of algebraic functions.  
 10. The method as claimed in claim 9, wherein said ratio of algebraic functions includes terms equivalent to:

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

5 11. The method as claimed in claim 10, wherein said nonlinear function includes a polynomial approximation of an  
arc-cosine function.

10 12. The method as claimed in claim 8, wherein each of said steps a) and b) are performed by a data processor under  
program control.

13. The method as claimed in claim 1, wherein:

- a plurality of analog signals are produced at a like plurality of locations within an electronic circuit, one location  
for each respective signal;
- the plurality of signals are applied to an analog multiplexer which has a like plurality of inputs, one for each  
respective signal, and which further has an analog output and a selection control input;
- the analog output is connected to an input of an analog-to-digital converter which has a digital output;
- the digital output is connected to an input port of a programmed data processor which has a first output port  
connected to the selection control input of the analog multiplexer;
- the programmed data processor has a second output port which is connected to an output unit for indicating  
an error condition to an operator; and
- the programmed data processor is programmed to:

25 1) output selection control signals to the analog multiplexer for conversion of each of the analog signals  
to a respective series of digital values by the analog-to-digital converter;

2) input into the programmed data processor the respective series of digital values for each of the analog  
signals;

30 3) determine an indication of amplitude and an indication of frequency of each of the analog signals by  
computing ratios of algebraic functions of at least four samples in the respective series of digital values  
for each of the analog signals; and

4) compare the indication of amplitude and the indication of frequency to limit values to indicate the error  
condition through the second output port when one of the indications of amplitude and frequency falls  
outside a boundary set by one of the limit values.

35 14. The method as claimed in claim 13, wherein said programmed data processor is programmed to compute said  
ratios of algebraic functions by computing a triplet of differences between successive values in each of said series  
of at least four samples, and by computing one of said ratios of algebraic functions indicative of amplitude from  
said triplet of differences, and computing one of said ratios of algebraic functions indicative of frequency from said  
triplet of differences.

40 15. The method as claimed in claim 14, wherein said programmed data processor is programmed to average together  
a plurality of said ratios of algebraic functions to compute said indication of amplitude, and to average together a  
plurality of said ratios of algebraic functions to compute said indication of frequency.

45 16. The method as claimed in claim 15, wherein said ratios of algebraic functions include algebraic functions which  
determine values for a denominator of each of said ratios of algebraic functions, and wherein said programmed  
data processor is programmed to exclude from said averages any ratios having a value for the denominator having  
a magnitude that is less than a limit value.

50 17. The method as claimed in claim 1, wherein each of said ratios has a denominator determined by a first one of said  
algebraic functions, and a numerator determined by a second one of said algebraic functions, and wherein said  
method further includes computing a value for said first one of said algebraic functions for each of said triplets,  
and excluding from said average any of said ratios for each of said triplets having a value for said first one of said  
algebraic functions that has a magnitude less than a threshold value.

55 18. The method as claimed in claim 17, wherein said threshold value is constant for each of said triplets.

19. The method as claimed in claim 17, wherein said threshold value is an average value of previously-computed

values for said first one of said algebraic functions

20. The method as claimed in claim 17, wherein said triplets are non-overlapping such that no two of said triplets both include any one of said sample values.

5 21. The method as claimed in claim 1, wherein the three samples values  $x_i$ ,  $x_{i-1}$ ,  $x_{i-2}$  in each of said triplets are computed from four sample values  $S_j$ ,  $S_{j-1}$ ,  $S_{j-2}$ ,  $S_{j-3}$  representing another signal, such that  $x_i$  is a difference between  $S_j$  and  $S_{j-1}$ ,  $x_{i-1}$  is a difference between  $S_{j-1}$  and  $S_{j-2}$ , and  $x_{i-2}$  is a difference between  $S_{j-2}$  and  $S_{j-3}$ .

10 22. The method as claimed in claim 1, further comprising the steps of comparing said average value to a predetermined limit value, and when said predetermined limit value is exceeded, reporting an error condition to an operator.

23. The method as claimed in claim 1, wherein said ratio includes terms equivalent to:

$$\frac{x_n^2(x_n^2 - x_{n+1}^2) x_{n-1}}{4x_n^2 - (x_{n+1}^2 + x_{n-1}^2)^2}$$

so that said ratio is an indication of amplitude of said sinusoidal signal.

20 24. The method as claimed in claim 1, wherein said ratio includes terms equivalent to:

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

so that said ratio is an indication of frequency of said sinusoidal signal

25 25. The method as claimed in claim 1, wherein the three samples values  $x_i$ ,  $x_{i-1}$ ,  $x_{i-2}$  in each of said triplets are computed from four sample values  $S_j$ ,  $S_{j-1}$ ,  $S_{j-2}$ ,  $S_{j-3}$ , representing another signal, such that  $x_i$  is a difference between  $S_j$  and  $S_{j-1}$ ,  $x_{i-1}$  is a difference between  $S_{j-1}$  and  $S_{j-2}$ , and  $x_{i-2}$  is a difference between  $S_{j-2}$  and  $S_{j-3}$  and wherein said ratio includes terms equivalent to:

$$\frac{x_n^3(x_n^2 - x_{n+1}^2 x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}$$

so that said ratio is an indication of amplitude of a sinusoidal signal, when said another signal represents said sinusoidal signal superimposed on a DC bias.

40 26. The method as claimed in claim 1, wherein each of steps a) and b) are performed by a data processor under program control.

#### 45 Patentansprüche

1. Ein Verfahren zum Erlangen und Einsetzen einer Angabe bzw. eines Anzeichens für eine Charakteristik eines sinusförmigen Signals, das einen Winkelgeschwindigkeitssensor (angular rate sensor) anregt, wobei das Verfahren die folgenden Schritte aufweist:

50 a) Erregen des Winkelgeschwindigkeitssensors mit dem sinusförmigen (sinusoidal) Signal;  
 b) Digitalisieren des sinusförmigen Signals in einem analog-zu-digital Wandler, wodurch eine Sequenz von Abtast- bzw. Samplewerten  $S_1, S_2, S_3, \dots, S_n$  an jeweiligen beabstandeten Zeitaugenblicken erzeugt wird;  
 c) Berechnen in einem Computer, der gemäß einer Software betrieben wird, einer Serie von Verhältnissen von algebraischen Funktionen von Dreiergruppen bzw. Triplets  $x_i, x_{i-1}, x_{i-2}$  von benachbarten Werten der Samplewerte;  
 d) Berechnen in einem Computer, der gemäß Software betrieben wird, eines Durchschnitts der Verhältnisse, um eine Angabe der Charakteristik zu erzeugen;

e) Anlegen der Angabe der Charakteristik an einen Korrektursignalgenerator, um ein Korrektursignal zu erzeugen; und  
 f) Subtrahieren, in einer Addiereinheit, des Korrektursignals von einem Winkelgeschwindigkeitssignal erzeugt durch den Winkelgeschwindigkeitssensor, um ein korrigiertes Winkelgeschwindigkeitssignal zu erzeugen.

5        2. Das Verfahren nach Anspruch 1, wobei  
       die Angabe der Charakteristik eine Schätzung (B) der Amplitude ist;  
       das Signal ein sinusförmiges Signal, dargestellt durch Samplewerte S1, S2, S3, S4 an jeweilig beabstandeten  
 10      Augenblicken ist;  
       die Anzahl der Samplewerte 4 ist; und x1 die Differenz zwischen S2 und S1, x2 die Differenz zwischen S3 und  
       S2, und x3 die Differenz zwischen S4 und S3 ist.

15      3. Das Verfahren nach Anspruch 2, wobei der Schritt des Berechnens einer Schätzung (B) der Amplitude ausgeführt  
       wird durch  
       i) Berechnen eines Verhältnisses der algebraischen Funktionen der Dreiergruppe der Differenzen x1, x2 und  
       x3; und durch  
       ii) Berechnen der Schätzung (B) der Amplitude als eine nicht lineare Funktion des Verhältnisses der algebrai-  
       schen Funktionen.

20      4. Das Verfahren nach Anspruch 3, wobei das Verhältnis der algebraischen Funktionen Terme beinhaltet, die äqui-  
       valent sind zu:

$$\frac{x_n^3(x_n^2 - x_{n+1}x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}$$

25      5. Das Verfahren nach Anspruch 4, wobei die nichtlineare Funktion eine Polynomnäherung einer Quadratwurzel-  
       funktion aufweist.

30      6. Das Verfahren nach Anspruch 2, wobei jede der Schritte a) und b) durch einen programmgesteuerten Datenpro-  
       zessor ausgeführt wird.

35      7. Verfahren nach Anspruch 2, das weiterhin den Schritt des Berechnens eines Korrekturwertes der Schätzung (B)  
       der Amplitude des sinusförmigen Signals aufweist um eine parasitäre bzw. Störkapazität in einer elektrischen  
       Schaltung zu kompensieren.

40      8. Verfahren nach Anspruch 1, wobei:  
       die Angabe der Charakteristik eine Schätzung (5) der Frequenz ist;  
       das Signal ein sinusförmiges Signal ist, das als abgetastete Werte S1, S2, S3, S4 an jeweiligen beabstandeten  
       Augenblicken bzw. Zeitpunkten dargestellt ist;  
       die Anzahl der Samplewerte 4 ist; und  
       x1 die Differenz zwischen S2 und S1, x2 die Differenz zwischen S3 und S2, und x3 die Differenz zwischen S4  
 45      und S3 ist.

50      9. Verfahren nach Anspruch 8, wobei der Schritt des Berechnens einer Schätzung (F) der Frequenz ausgeführt wird  
       durch  
       i) Berechnen eines Verhältnisses von algebraischen Funktionen der Differenzen x1, x2 und x3; und  
       ii) Berechnen der Schätzung (F) der Frequenz als eine nichtlineare Funktion des Verhältnisses der algebrai-  
       schen Funktionen.

55      10. Verfahren nach Anspruch 9, wobei das Verhältnis der algebraischen Funktionen Terme aufweist, die äquivalent  
       sind zu:

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

5     11. Verfahren nach Anspruch 10, wobei die nichtlineare Funktion eine Polynomnäherung einer Arcuscosinusfunktion aufweist.

10    12. Verfahren nach Anspruch 8, wobei jeder der Schritte a) und b) durch einen programmgesteuerten Datenprozessor ausgeführt wird.

10    13. Verfahren nach Anspruch 1, wobei:

15       eine Vielzahl von Analogsignalen an einer gleich großen Vielzahl von Positionen innerhalb eines elektronischen Schaltkreises erzeugt werden, jeweils eine Position für jedes jeweilige Signal;

15       die Vielzahl der Signale an einem Analogmultiplexer angelegt werden, der eine gleich große Anzahl von Eingängen hat, jeweils einen für jedes jeweilige Signal, und der weiterhin einen analogen Ausgang und einen Auswahlsteuereingang hat;

20       der Analogausgang mit einem Eingang eines analog-zu-digital Wandlers verbunden ist, der einen digitalen Ausgang hat;

20       die digitale Ausgabe verbunden ist mit einem Eingangsanschluss eines programmierten Datenprozessors, der einen ersten Ausgangsanschluss hat, der verbunden ist mit dem Auswahlsteuereingang des Analogmultiplexers;

25       der programmierte Datenprozessor einen zweiten Ausgangsanschluss hat, der verbunden ist mit einer Ausgabeeinheit zum Anzeigen eines Fehlerzustands an einen Betreiber; und

25       der programmierte Datenprozessor programmiert ist zum:

30       1) Ausgeben von Auswahlsteuersignalen zu dem Analogmultiplexer für die Konvertierung eines jeden der Analogsignale in eine jeweilige Serie von digitalen Werten durch den analog-zu-digital Wandler;

30       2) Eingeben der jeweiligen Serien von digitalen Werten in den programmierten Datenprozessor für jedes der Analogsignale;

35       3) Bestimmen einer Angabe der Amplitude und einer Eingabe der Frequenz für jedes der Analogsignale durch Berechnen von Verhältnissen von algebraischen Funktionen von zumindest vier Samples in den jeweiligen Serien von digitalen Werten für jedes der Analogsignale; und

35       4) Vergleichen der Angaben der Amplitude und der Angabe der Frequenz mit Grenzwerten, um den Fehlerzustand über den zweiten Ausgabeanchluss anzuzeigen, wenn eine der Angaben der Amplitude und der Frequenz außerhalb der Grenze, die durch die Grenzwerte gesetzt wird, liegt.

40    14. Verfahren nach Anspruch 13, wobei der programmierte Datenprozessor programmiert ist zum Berechnen der Verhältnisse der algebraischen Funktionen durch Berechnung einer Dreiergruppe von Differenzen zwischen aufeinanderfolgenden Werten in jeder der Serie von zumindest vier Samples und durch Berechnen eines der Verhältnisse der algebraischen Funktionen anzeigen für die Amplitude aus der Dreiergruppe der Differenzen, und Berechnen eines der Verhältnisse der algebraischen Funktionen anzeigen für die Frequenz aus der Dreiergruppe der Differenzen.

45    15. Verfahren nach Anspruch 14, wobei der programmierte Datenprozessor programmiert ist zum Mitteln bzw. Durchschnittsbilden einer Vielzahl der Verhältnisse der algebraischen Funktionen, um die Angabe der Amplitude zu berechnen, und zum Mitteln einer Vielzahl von den Verhältnissen der algebraischen Funktionen, um eine Angabe der Frequenz zu berechnen.

50    16. Verfahren nach Anspruch 15, wobei die Verhältnisse von algebraischen Funktionen algebraische Funktionen aufweisen, die Werte für einen Nenner für jedes der Verhältnisse von algebraischen Funktionen bestimmen, und wobei der programmierte Datenprozessor so programmiert ist, daß er von den Durchschnitten alle Verhältnisse ausschließt, die einen Wert für den Nenner bzw. Divisor haben, dessen Betrag geringer ist als ein Grenzwert.

55    17. Verfahren nach Anspruch 1, wobei jedes der Verhältnisse einen Divisor hat, der durch eine erste der algebraischen Funktionen bestimmt ist, und einen Zähler hat, der durch eine zweite der algebraischen Funktionen bestimmt ist, und wobei das Verfahren weiterhin aufweist, dass ein Wert für die erste der algebraischen Funktionen für jede der Dreiergruppen berechnet wird und weiter von dem Durchschnitt all die Verhältnisse für jede der Dreiergruppen

ausschließt, die einen Wert für die erste der algebraischen Funktionen haben, einen Betrag kleiner als ein Schwellenwert hat.

18. Verfahren nach Anspruch 17, wobei der Schwellenwert für jede Dreiergruppe konstant ist.

5 19. Verfahren nach Anspruch 17, wobei der Schwellenwert ein Durchschnittswert von zuvor berechneten Werten für die erste der algebraischen Funktionen ist.

10 20. Verfahren nach Anspruch 17, wobei die Dreiergruppen sich nicht überlappen, so dass keine zwei der Dreiergruppen beide einen gleichen Abtastungswert beinhalten.

15 21. Verfahren nach Anspruch 1, wobei die drei Samplewerte  $x_i, x_{i-1}, x_{i-2}$  in jeder der Dreiergruppen aus vier Abtastwerten  $S_j, S_{j-1}, S_{j-2}, S_{j-3}$ , die ein weiteres Signal darstellen, berechnet werden, so dass  $x_i$  eine Differenz zwischen  $S_j$  und  $S_{j-1}$ ,  $x_{i-1}$  eine Differenz zwischen  $S_{j-1}$  und  $S_{j-2}$ , und  $x_{i-2}$  eine Differenz zwischen  $S_{j-2}$  und  $S_{j-3}$  ist.

22. Verfahren nach Anspruch 1, das weiterhin die Schritte des Vergleichens des Durchschnittswertes mit einem vorbestimmten Grenzwert und Berichten eines Fehlerzustandes an einen Betreiber aufweist, wenn der vorbestimmte Grenzwert überschritten wird.

20 23. Verfahren nach Anspruch 1, wobei das Verhältnis Terme aufweist, die äquivalent sind zu:

$$\frac{x_n^2(x_n^2 - x_{n+1}^2) x_{n-1}}{4x_n^2 - (x_{n+1} + x_{n-1})^2}$$

25 so dass das Verhältnis eine Angabe über die Amplitude des sinusförmigen Signals ist.

24. Verfahren nach Anspruch 1, wobei das Verhältnis Terme aufweist, die äquivalent sind zu:

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

35 so dass das Verhältnis eine Angabe über die Frequenz des sinusförmigen Signals ist.

25 26. Verfahren nach Anspruch 1, wobei die drei Samplewerte  $x_i, x_{i-1}, x_{i-2}$  in jeder der Dreiergruppen aus vier Samplewerten  $S_j, S_{j-1}, S_{j-2}, S_{j-3}$ , die ein weiteres Signal darstellen, berechnet werden, so dass  $x_i$  eine Differenz zwischen  $S_j$  und  $S_{j-1}$ ,  $x_{i-1}$  eine Differenz zwischen  $S_{j-1}$  und  $S_{j-2}$ , und  $x_{i-2}$  eine Differenz zwischen  $S_{j-2}$  und  $S_{j-3}$  ist, und wobei das Verhältnis Terme aufweist, die äquivalent sind zu:

$$\frac{x_n^3(x_n^2 - x_{n+1}^2 x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}$$

45 so dass das Verhältnis eine Angabe der Amplitude eines sinusförmigen Signals ist, wenn das weitere Signal das sinusförmige Signal überlagert auf ein DC-Bias darstellt.

50 26. Verfahren nach Anspruch 1, wobei jeder der Schritte a) und b) durch einen programmgesteuerten Datenprozessor ausgeführt wird.

#### Revendications

55 1. Procédé d'obtention et d'utilisation d'une indication d'une caractéristique d'un signal sinusoïdal excitant un capteur de vitesse angulaire, ledit procédé comprenant les étapes consistant à :

a) exciter ledit capteur de vitesse angulaire avec ledit signal sinusoïdal ;  
 b) numériser ledit signal sinusoïdal dans un convertisseur analogique/ numérique, produisant ainsi une sé-

quence de valeurs d'échantillonnage S1, S2, S3, ... Sn à des instants temporels espacés respectifs ;  
 c) calculer dans un ordinateur fonctionnant conformément à un logiciel une série de rapports de fonctions algébriques de triplet xi, xi-1, xi-2 de valeurs voisines desdites valeurs d'échantillonnage ;  
 5 d) calculer dans un ordinateur fonctionnant conformément à un logiciel une moyenne desdits rapports pour produire ladite indication de ladite caractéristique ;  
 e) appliquer ladite indication de ladite caractéristique à un générateur de signaux de correction pour produire un signal de correction ; et  
 f) soustraire, dans une unité d'additionneur, le signal de correction d'un signal de vitesse angulaire généré par ledit capteur de vitesse angulaire pour produire un signal de vitesse angulaire corrigé.

10 2. Procédé selon la revendication 1, dans lequel :

- l'indication de la caractéristique est une estimation (B) de l'amplitude ;
- le signal est un signal sinusoïdal représenté comme des valeurs d'échantillonnage S1, S2, S3, S4 à des instants temporels espacés respectifs ;
- le nombre de valeurs d'échantillonnage s'élève à quatre ; et
- x1 est la différence entre S2 et Si, x2 est la différence entre S3 et S2 et x3 est la différence entre S4 et S3.

15 20 3. Procédé selon la revendication 2, dans lequel ladite étape de calcul d'une estimation (B) de ladite amplitude est effectuée en

- i) calculant un rapport de fonctions algébriques dudit triplet de différences x1, x2 et x3 ; et
- ii) calculant ladite estimation (B) de ladite amplitude comme une fonction non linéaire dudit rapport de fonctions algébriques.

25 4. Procédé selon la revendication 3, dans lequel ledit rapport de fonctions algébriques comprend des termes équivalents à :

$$\frac{x_n^3(x_n^2 - x_{n+1}x_{n-1})}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}$$

30 35 5. Procédé selon la revendication 4, dans lequel ladite fonction non linéaire comprend une approximation polynomiale d'une fonction de racine carrée.

40 35 6. Procédé selon la revendication 2, dans lequel chacune desdites étapes a) et b) est effectuée par un processeur de données sous le contrôle d'un programme.

45 7. Procédé selon la revendication 2, comprenant en outre l'étape de calcul d'une valeur de correction à partir de ladite estimation (B) de l'amplitude dudit signal sinusoïdal pour compenser une capacité parasite dans un circuit électrique.

50 8. Procédé selon la revendication 1, dans lequel :

- l'indication de la caractéristique est une estimation (F) de la fréquence ;
- le signal est un signal sinusoïdal représenté comme des valeurs d'échantillonnage S1, S2, S3, S4 à des instants temporels espacés respectifs ;
- le nombre de valeurs d'échantillonnage s'élève à quatre ; et
- x1 est la différence entre S2 et Si, x2 est la différence entre S3 et S2 et x3 est la différence entre S4 et S3.

55 9. Procédé selon la revendication 8, dans lequel ladite étape de calcul d'une estimation (F) de ladite fréquence est effectuée en

- i) calculant un rapport de fonctions algébriques desdites différences x1, x2 et x3 ; et
- ii) calculant ladite estimation (F) de ladite fréquence comme une fonction non linéaire dudit rapport de fonctions algébriques.

10. Procédé selon la revendication 9, dans lequel ledit rapport de fonctions algébriques comprend des termes équi-

valents à :

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

5

11. Procédé selon la revendication 10, dans lequel ladite fonction non linéaire comprend une approximation polynomiale d'une fonction d'arc cosinus.

10 12. Procédé selon la revendication 8, dans lequel chacune desdites étapes a) et b) est effectuée par un processeur de données sous le contrôle d'un programme.

13. Procédé selon la revendication 1, dans lequel :

15 - une pluralité de signaux analogiques est produite à une pluralité identique d'emplacements à l'intérieur d'un circuit électronique, avec un emplacement pour chaque signal respectif ;  
 - la pluralité de signaux est appliquée à un multiplexeur analogique qui comporte une pluralité identique d'entrées, une pour chaque signal respectif, et qui comporte en outre une sortie analogique et une entrée de commande de sélection ;  
 20 - la sortie analogique est connectée à une entrée d'un convertisseur analogique/ numérique qui comporte une sortie numérique ;  
 - la sortie numérique est connectée à un port d'entrée d'un processeur de données programmé dont un premier port de sortie est connecté à l'entrée de commande de sélection du multiplexeur analogique ;  
 - le processeur de données programmé comporte un deuxième port de sortie qui est connecté à une unité de sortie pour indiquer une condition d'erreur à un opérateur ; et  
 25 - le processeur de données programmé est programmé pour :

30 1) délivrer des signaux de commande de sélection au multiplexeur analogique pour faire convertir chacun des signaux analogiques en une série respective de valeurs numériques par le convertisseur analogique/ numérique ;  
 2) entrer dans le processeur de données programmé la série respective de valeurs numériques pour chacun des signaux analogiques ;  
 3) déterminer une indication d'amplitude et une indication de fréquence pour chacun des signaux analogiques en calculant des rapports de fonctions algébriques d'au moins quatre échantillons dans la série respective de valeurs numériques pour chacun des signaux analogiques ; et  
 35 4) comparer l'indication d'amplitude et l'indication de fréquence à des valeurs limites pour indiquer la condition d'erreur à travers le deuxième port de sortie quand l'une des indications d'amplitude et de fréquence tombe en dehors d'une borne définie par l'une des valeurs limites.

40 14. Procédé selon la revendication 13, dans lequel ledit processeur de données programmé est programmé pour calculer lesdits rapports de fonctions algébriques en calculant un triplet de différences entre des valeurs successives de chacun de la série d'au moins quatre échantillons, et en calculant l'un desdits rapports de fonctions algébriques indiquant l'amplitude à partir dudit triplet de différences et en calculant l'un desdits rapports de fonctions algébriques indiquant la fréquence à partir dudit triplet de différences.

45 15. Procédé selon la revendication 14, dans lequel ledit processeur de données programmé est programmé pour établir la moyenne d'une pluralité desdits rapports de fonctions algébriques pour calculer ladite indication d'amplitude, et pour établir la moyenne d'une pluralité desdits rapports de fonctions algébriques pour calculer ladite indication de fréquence.

50 16. Procédé selon la revendication 15, dans lequel lesdits rapports de fonctions algébriques comprennent des fonctions algébriques qui déterminent des valeurs pour un dénominateur de chacun desdits rapports de fonctions algébriques, et dans lequel ledit processeur de données programmé est programmé pour exclure desdites moyennes tous les rapports comportant une valeur pour le dénominateur ayant une grandeur qui est inférieure à une valeur limite.

55 17. Procédé selon la revendication 1, dans lequel chacun desdits rapports comporte un dénominateur déterminé par une première desdites fonctions algébriques, et un numérateur déterminé par une deuxième desdites fonctions

algébriques, et dans lequel ledit procédé comprend en outre le calcul d'une valeur pour ladite première desdites fonctions algébriques pour chacun desdits triplets, et l'exclusion de ladite moyenne de tout rapport desdits rapports pour chacun desdits triplets ayant une valeur pour ladite première fonction desdites fonctions algébriques qui a une grandeur inférieure à une valeur de seuil.

5                   18. Procédé selon la revendication 17, dans lequel ladite valeur de seuil est constante pour chacun desdits triplets.

10                 19. Procédé selon la revendication 17, dans lequel ladite valeur de seuil est une valeur moyenne de valeurs calculées auparavant pour ladite première fonction desdites fonctions algébriques.

15                 20. Procédé selon la revendication 17, dans lequel lesdits triplets ne se recouvrent pas de sorte que deux desdits triplets n'incluent jamais à la fois l'une quelconque desdites valeurs d'échantillonnage.

20                 21. Procédé selon la revendication 1, dans lequel les trois valeurs d'échantillonnage  $x_i, x_{i-1}, x_{i-2}$  dans chacun desdits triplets sont calculées à partir de quatre valeurs d'échantillonnage  $S_j, S_{j-1}, S_{j-2}, S_{j-3}$  qui représentent un autre signal, de sorte que  $x_i$  est une différence entre  $S_j$  et  $S_{j-1}$ ,  $x_{i-1}$  est une différence entre  $S_{j-1}$  et  $S_{j-2}$  et  $x_{i-2}$  est une différence entre  $S_{j-2}$  et  $S_{j-3}$ .

25                 22. Procédé selon la revendication 1, comprenant en outre les étapes consistant à comparer ladite valeur moyenne à une valeur limite prédéterminée, et quand ladite valeur limite prédéterminée est dépassée, signaler une condition d'erreur à un opérateur.

23. Procédé selon la revendication 1, dans lequel ledit rapport comprend des termes équivalents à :

$$\frac{x_n^2(x_{n-1}^2 - x_{n+1}^2)}{4x_n^2 - (x_{n+1}^2 + x_{n-1}^2)^2}$$

30                 de sorte que ledit rapport est une indication d'amplitude dudit signal sinusoïdal.

35                 24. Procédé selon la revendication 1, dans lequel ledit rapport comprend des termes équivalents à :

$$\frac{x_{n+1} + x_{n-1}}{x_n}$$

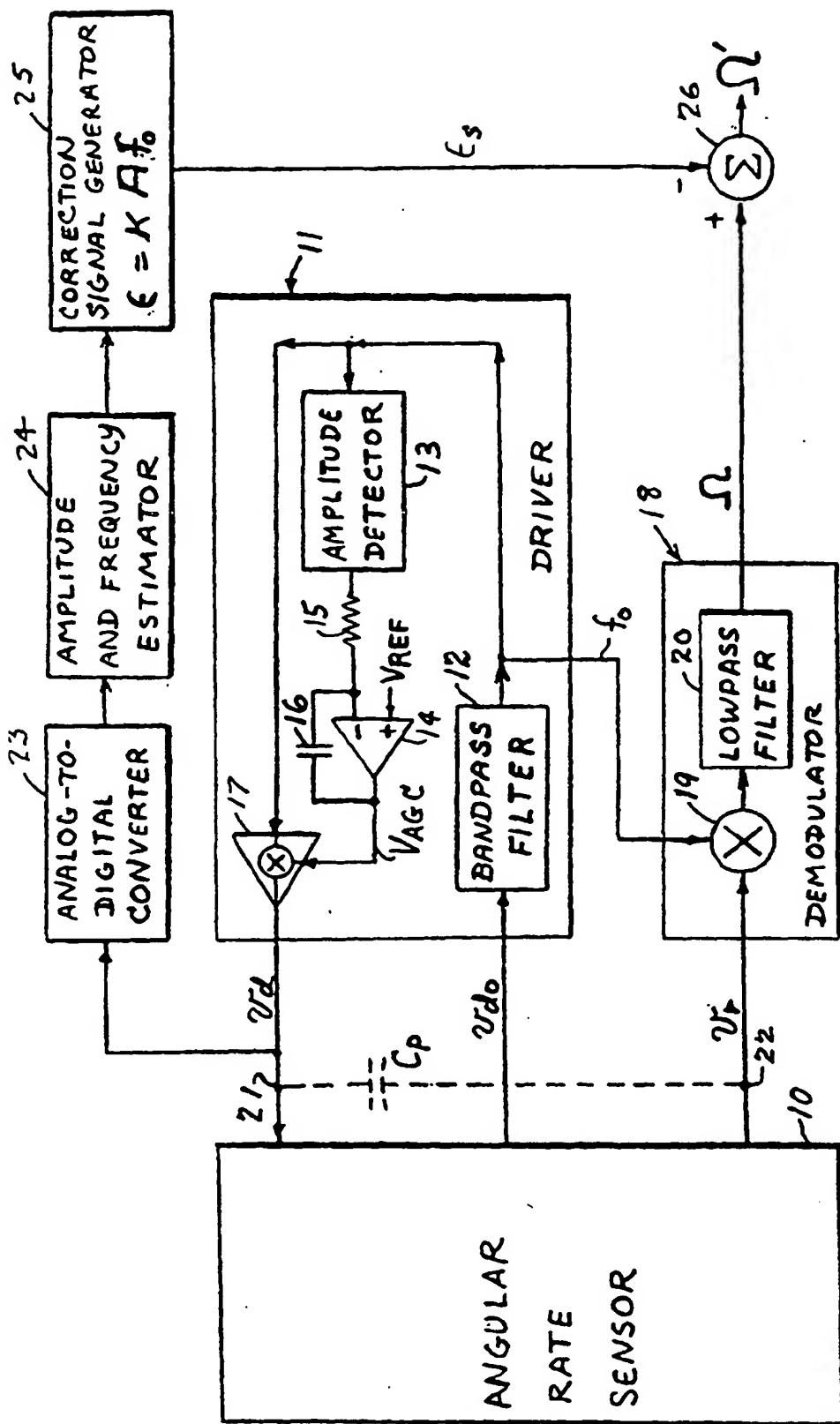
40                 de sorte que ledit rapport est une indication de fréquence dudit signal sinusoïdal.

45                 25. Procédé selon la revendication 1, dans lequel les trois valeurs d'échantillonnage  $x_i, x_{i-1}, x_{i-2}$  dans chacun desdits triplets sont calculées à partir de quatre valeurs d'échantillonnage  $S_j, S_{j-1}, S_{j-2}, S_{j-3}$  qui représentent un autre signal, de sorte que  $x_i$  est une différence entre  $S_j$  et  $S_{j-1}$ ,  $x_{i-1}$  est une différence entre  $S_{j-1}$  et  $S_{j-2}$  et  $x_{i-2}$  est une différence entre  $S_{j-2}$  et  $S_{j-3}$  ; et dans lequel le rapport comprend des termes équivalents à :

$$\frac{x_n^3(x_{n-1}^2 - x_{n+1}^2) x_{n-1}}{[2x_n - (x_{n+1} + x_{n-1})]^2 [(2x_n) + (x_{n+1} + x_{n-1})]}$$

50                 de sorte que ledit rapport est une indication d'amplitude d'un signal sinusoïdal quand ledit autre signal représente ledit signal sinusoïdal superposé à une polarisation en courant continu.

55                 26. Procédé selon la revendication 1, dans lequel chacune des étapes a) et b) est effectuée par un processeur de données sous le contrôle d'un programme.



# FIG. 1

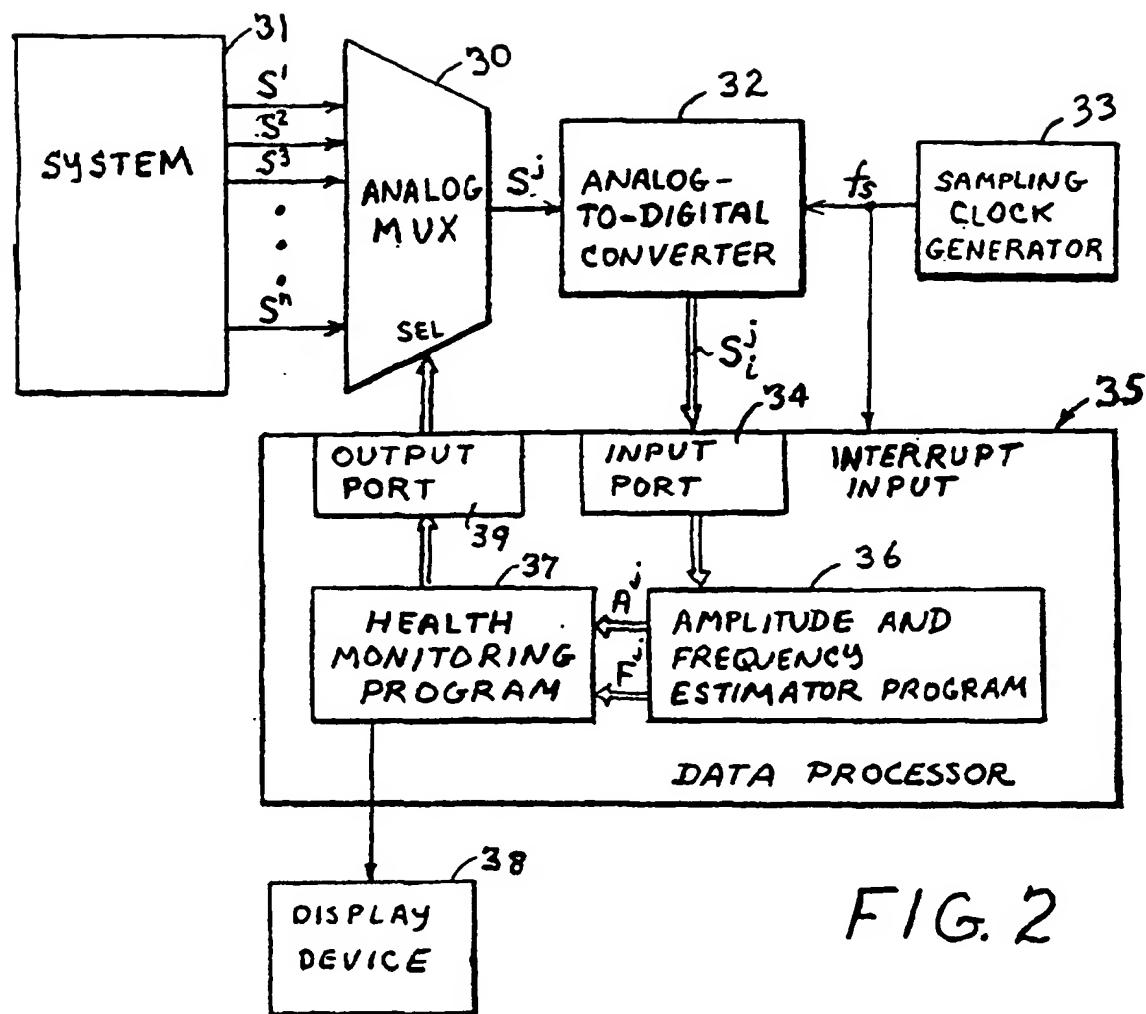


FIG. 2

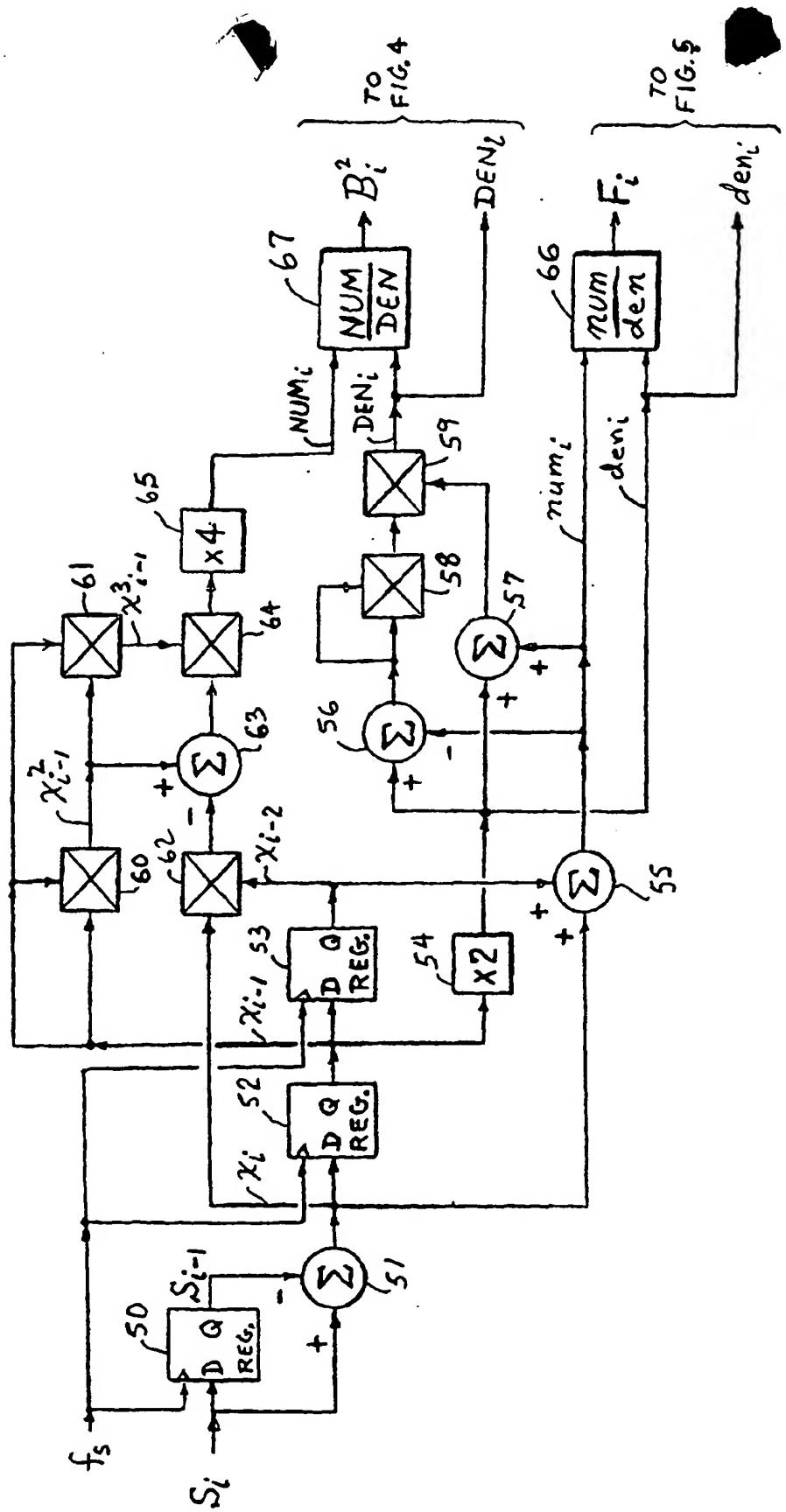


FIG. 3

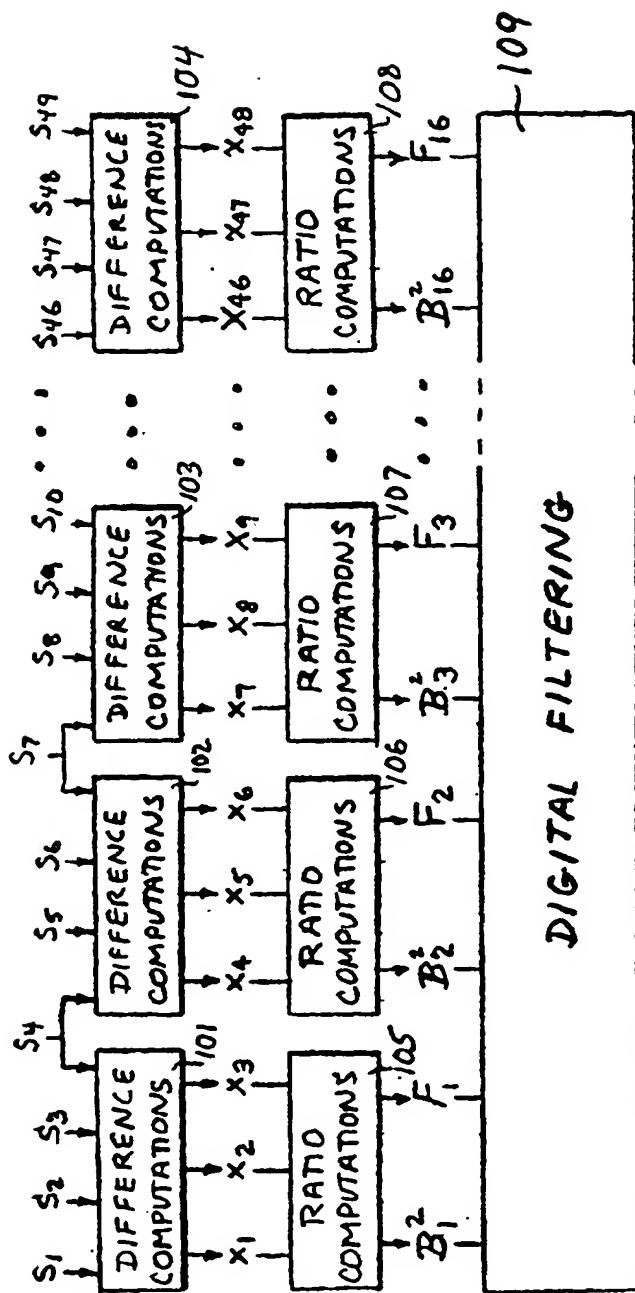
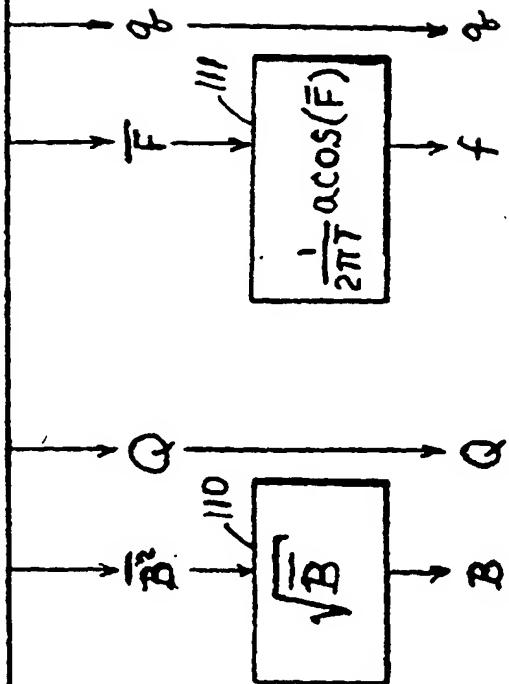


FIG. 6



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